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Hussein ZAHR, Franck SCUILLER, Eric SEMAIL - Five-phase SPM machine with electronic pole changing effect for marine propulsion - In: ESARS, France, 2016-11 - ESARS - 2016

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Five-phase SPM machine with electronic pole changing effect for marine propulsion

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Abstract—In this paper, the possibility of designing a five-phase Surface-mounted Permanent Magnet (SPM) machine with 20 slots and 8 poles for a low power marine propulsion system is examined. Due to its particular winding and surface magnet design, the machine inherently offers an electronic pole changing effect from 3×4 pole pairs at low speed to 4 pole pairs at high speed. At high speed, in the constant power range, according to Finite Element Analysis, the Maximum Torque Per Ampere strategy appears not to be the right solution to minimize the whole machine losses (copper, iron and magnets). In particular, a strategy that favors the 4-pole rotating field at high speed allows to mitigate the magnet losses, thus limiting the risk of magnet overheating.

Index Terms—Multi-phase machine, permanent magnets, magnet losses, iron losses, fractional-slot winding

I. NOMENCLATURE

SPM	Surface-mounted Permanent Magnet
FEA	Finite Elements Analysis
CPR	Constant Power Range
MM	Main Machine (1st harmonic dq-subspace)
SM	Secondary Machine (3rd harmonic dq-subspace)
Ω_m	Mechanical speed (rad/s)
p	Pole pair number
R	Armature resistance
ϵ_1, ϵ_3	MM and SM no load back-emf at 1 rad/s
L_1, L_3	MM and SM cyclic inductances
θ_1, θ_3	MM and SM back-emf to current angles
I_1, I_3	MM and SM currents
V_b, I_b	Base RMS voltage and current
Ω_b, T_b	Base speed and torque

II. INTRODUCTION

Multi-phase motors are widely used in electrical marine propulsion for reasons such as reliability, smooth torque and distribution of power [1]. For low power propulsion system (less than 10kW), the power partition constraint results from the low DC voltage (less than 60V) that supplies the drive. Hence increasing the phase number allows to limit the rating of the power electronic components. In addition, compactness objective can be more easily achieved if the phase number is considered as a design parameter. For instance, with five-phase machine, third harmonic current injection can be performed to boost the torque [2], [3]. Regarding the rotor, Permanent Magnet (PM) structure contribute to

enhance the power density. In case of Surface-mounted Permanent Magnet (SPM) rotor, the ripple torque mitigation is facilitated. Furthermore, with five-phase SPM machine, third harmonic current injection can be used to eliminate the pulsating torque [4]. If fractional-slot windings facilitate the reduction of cogging torque for SPM machine [5], they also generate magnetomotive force harmonics that could result in excessive magnet losses. Machine with 0.5 slots per phase and per pole ($s_{pp} = 0.5$) are known to limit this effect [6]. In addition, the slot filling can also be improved with this solution [7]. Therefore the machine here considered is a five-phase machine with 20 slots and 8 poles (20-8-5 configuration) for a marine propeller.

The 3-phase counterpart of this 20-8-5 machine has 8 poles and 12 slots (12-8-3 configuration). With reference to this 12-8-3 machine, the benefits of the 20-8-5 machine are examined in [8] for the same design specifications: rated torque, power and external diameters are identical. With numerical computations of the two machines, this study shows that the 5-phase configuration allows a significant reduction of the magnet losses. In addition, the 5-phase machine facilitates the reduction of the ripple torques (cogging and pulsating) that is of critical importance at low speed.

This paper focuses on another property of the 20-8-5 machine. Due to its particular winding distribution, this machine inherently owns 3×4 pairs of pole and 4 pairs of pole. Hence an electronic pole changing effect can be obtained if the machine is designed to operate at low speed with 3×4 pole pairs or at high speed with 4 pole pairs. More generally the appropriate polarity has to be selected regarding the load demand in transient or steady state, taking into account the inverter rating and the efficiency or torque quality requirements. Pole changing methods by winding switching are well known for induction machine [9]. For multiphase induction machine, pole phase modulation strategy can be applied [10]. In [11], the speed range of a five-phase PM machine is extended by switching between different stator configurations. A similar procedure is achieved in [12] but with electronic switching. In this paper, the pole changing effect is electronically ensured by the inverter, depending of the levels of first and third harmonics of current.

The paper is divided into two parts. In the first part, the

20-8-5 machine design is introduced. The magnet layer to obtain the double polarity property is introduced. To master the sizing, numerical field calculations are reported and the torque/speed characteristic is estimated. The second part focuses on the control strategy in the constant power range that corresponds to the steady state operation of the propeller. Two strategies are described and compared regarding the copper, magnet and iron losses (estimated with FEA).

III. MACHINE DESIGN

A. Five-phase machine modeling

If the magnetic saturation and the demagnetization issue are not considered, it can be shown that a star-connected five-phase SPM machine behaves as two two-phase virtual machines that are magnetically independent but electrically and mechanically coupled [13]. Furthermore, as the rotor saliency can be neglected with SPM machines, the space harmonics are distributed among the two virtual machines: the virtual machine sensitive to the fundamental is called Main Machine (MM) whereas the other sensitive to the third harmonic is called Secondary Machine (SM). Actually the virtual machine is a physical reading of the mathematical subspace build on the linear application that describes the phase-to-phase magnetic couplings: this two-dimension subspace is usually represented with $\alpha\beta$ -axis circuit in stationary frame or with dq -axis circuit in rotating frame. As there is no saliency effect, no distinction has to be made between d-axis and q-axis inductance.

B. Design specifications

The machine is intended to be integrated in a pod for an electrical outboard. The propeller is driven by the electrical machine with a mechanical gear that reduces the electrical rotating speed by five. The main machine parameters are listed in table I.

TABLE I
PARAMETERS FOR THE CONSIDERED MACHINE

Rated Em power	$P_{em} = 7.7kW$
Constant Speed Range	$[2250rpm - 4500rpm]$
Rated Em Torque	$T_{em,r} = 34.0Nm$
DC voltage	$V_{dc} = 30V$
Base current	$I_b = 290A$
Pole pair number	$p = 4$
Slot number per phase per pole	$s_{pp} = 0.5$
Effective length	$L_m = 0.0923m$
External diameter	$D_{ext} = 0.209m$
Stator diameter	$2R_s = 0.1444m$
Stator yoke thickness	$t_{ys} = 0.011m$
Mechanical airgap	$g = 0.001m$
Rotor yoke thickness	$t_{yr} = 0.011m$
Magnet layer thickness	$h_m = 3g$
Remanent flux density	$B_r = 1.17T$
Slot width (τ_s , tooth pitch)	$0.5\tau_s$
Slot width opening	$0.25\tau_s$
Slot-closing thickness	$t_{sc} = 0.001m$
Slot depth	$d_s = 0.0205m$
Linear load	$A_L = 25.6 \times 10^3 A/m$
Current density	$j_s = 5 \times 10^6 A/m^2$

The electromagnetic circuit is sketched out in Fig.1 (over a pole pair): the five-phase winding distribution with the corresponding first and third harmonic winding factors ($k_{w,1}$ and $k_{w,3}$) can be observed. The magnet layer shape is arranged to make the two virtual machines enable to produce the same torque level. To reach this goal, the rotor pole consists of two radially magnetized magnets, each magnet covering one third of the pole arc, as illustrated by Fig.1.

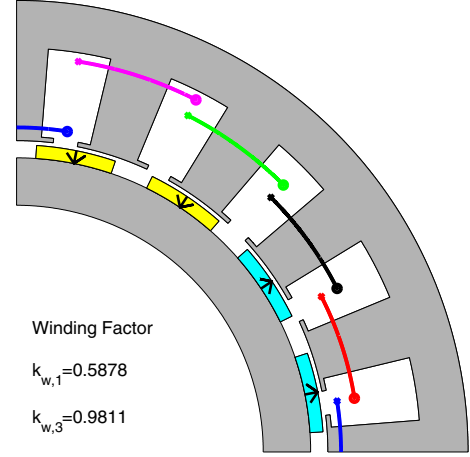


Fig. 1. Electromagnetic circuit of the 5-phase machine

C. Field analysis

In this subsection, the electromagnetic behaviour of the machine is estimated with FEA software *FEMM* [14] under magnetostatic hypothesis. In addition, saturation effects are not taken into account (linear assumption for the materials).

Fig.2 shows the no-load back-emf waveform and spectrum. The double polarity of the machine can be inferred. The spectrum confirms that first and third harmonic terms are of the same order.

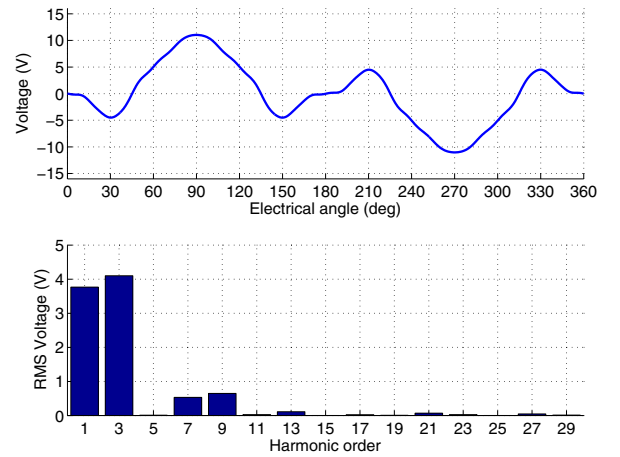


Fig. 2. No load back-emf at 2250rpm mechanical speed (FEA)

The inductance values L_1 for the MM and L_3 for the SM are calculated by loading the machine with the rated current:

- $L_1 = 3.1mH$ for the MM (4 pole pairs)

- $L_3 = 4.0mH$ for the SM (3×4 pole pairs).

Fig.3 shows the flux lines when loading the machine with fundamental rated current (for a given rotor position). The field intensity values allow to control the right sizing of the electromagnetic circuit: in the yokes and in the stator teeth, the field intensity is lower than 1.4T. Fig.4 focuses on the cogging torque estimation. As previous, the cogging torque is negligible: its amplitude is less than 0.25Nm, that is less than 1% the rated torque.

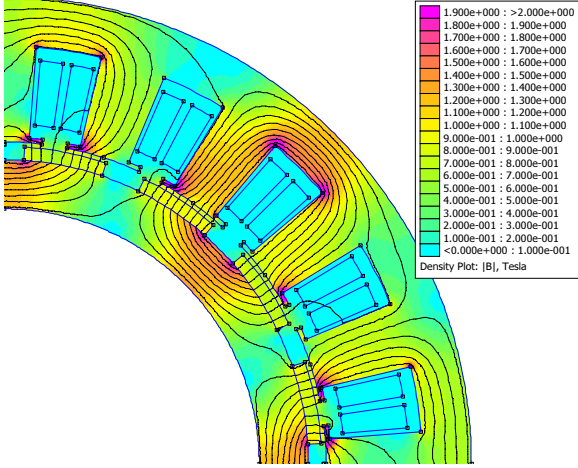


Fig. 3. Flux density (for fundamental rated current)

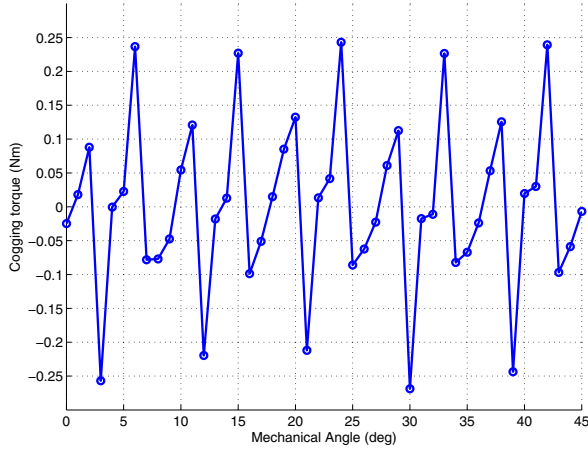


Fig. 4. Cogging torque estimation (FEA)

D. Maximum reachable torque for finite Volt-Ampere rating

In this subsection, the torque/speed characteristic of the machine is calculated: for a given mechanical speed Ω_m (i.e. for a given electrical speed ω), taking into account the maximum DC voltage and the maximum copper losses (driven by base current I_b), the goal consists in finding the MM and SM current distribution that maximizes the electromagnetic torque [15]. To solve this problem is equivalent to find the optimal d-axis and q-axis references for each virtual machine. The Maximum Torque Per Ampere (MTPA) for a given speed

is then obtained. The optimization variable is defined as follows:

$$z = [I_1 \quad \theta_1 \quad I_3 \quad \theta_3]^T \quad (1)$$

The optimization variable is lower and upper bounded according to the following relations:

$$Z_{low} = \begin{bmatrix} 0 \\ -\pi \\ 0 \\ -\pi \end{bmatrix} \leq z \leq \begin{bmatrix} I_b \\ \pi \\ I_b \\ \pi \end{bmatrix} = Z_{up} \quad (2)$$

The objective is to maximize the electromagnetic torque. This goal is expressed in the following relation where T is the average electromagnetic torque:

$$z^* = \operatorname{argmin}(-T(z)) \quad (3)$$

The average electromagnetic torque is the sum of the torque of each virtual machine. The MM torque (due to the fundamental of current) is denoted T_1 and the SM torque (due to the third harmonic of current) is denoted T_3 :

$$T_1 = 5\epsilon_1 I_1 \cos \theta_1 \quad (4)$$

$$T_3 = 5\epsilon_3 I_3 \cos \theta_3 \quad (5)$$

The five-phase machine torque is then expressed as follows:

$$T = 5\epsilon_1 I_1 \cos \theta_1 + 5\epsilon_3 I_3 \cos \theta_3 \quad (6)$$

Equation (6) is used in relation (3) to track the optimal current repartition z^* . The non linear constraint regarding the peak phase voltage is written in the following relation:

$$f_V(z) = \max \{v(p\Omega_m t, z), p\Omega_m t \in [0..2\pi]\} - V_{peak} \quad (7)$$

In equation (7), $v(p\Omega_m t, z)$ is the machine phase-to-neutral voltage for the current determined by z at Ω_m speed. It should be noted that the considered voltage contains all the harmonics (i.e. not only the first and the third harmonics). The maximum allowable peak voltage is chosen to be half the bus voltage (thus meaning that linear modulation operation is targeted):

$$V_{peak} = \frac{V_{dc}}{2} \quad (8)$$

The constraint relative to the maximum RMS current is defined by the following equation:

$$f_I(z) = z(1)^2 + z(3)^2 - I_b^2 \quad (9)$$

The following expression summarizes the optimization problem under consideration:

$$\begin{aligned} z^* &= \operatorname{argmin}(-T(z)) \\ \text{with } &\begin{cases} Z_{low} \leq z \leq Z_{up} \\ f_V(z) \leq 0 \\ f_I(z) \leq 0 \end{cases} \end{aligned} \quad (10)$$

Fig.5 shows the resulting torque/speed characteristic corresponding to the resolution of optimization problem (10). It can be observed that the rated torque (about 34Nm) is obtained by using the virtual MM and the virtual SM in the same time, thus meaning that the five-phase machine

here considered is designed to operate with first and third harmonic of current. In addition, the electronic pole changing effect is obtained since, at low speed, the MM (3×4 poles) mainly contributes to the torque whereas, at high speed, the SM (4 poles) torque becomes higher. The iso-power line (7.7kW) drawn in fig.5 allows to determine the constant power range that is between 2250rpm and 4500rpm (as specified in table I).

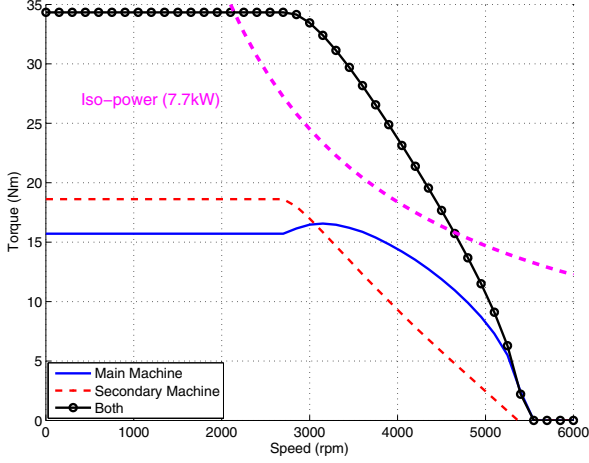


Fig. 5. Maximum reachable torque for the five-phase machine

IV. CONTROL STRATEGIES IN THE CONSTANT POWER RANGE

This section focuses on the machine operation in the CPR. At low speed (below 2250rpm), the machine is supposed being in transient states and the MTPA strategy previously introduced is performed. At high speeds (between 2250rpm and 4500rpm), the constant power control is used: in this mode, since the torque is not maximized, the constant power can be obtained with different current distributions, depending on the considered objective. Therefore, two objectives will be examined: one that aims to reduce the copper losses and another that aims to maximize the MM torque contribution. These two strategies will be compared regarding the machine losses with FEA.

A. Constant Power Control with minimizing copper losses

For the control here described, the goal consists in minimizing the copper losses for a given electromagnetic power accounting the maximum allowable peak voltage. For a given torque, as the copper losses are minimized, this strategy is actually a MTPA one and is called CPR-MTPA in the following. The optimization problem can be written as follows:

$$\begin{aligned} z^* &= \operatorname{argmin}(z(1)^2 + z(3)^2) \\ \text{with } &\begin{cases} Z_{low} \leq z \leq Z_{up} \\ f_V(z) \leq 0 \\ f_T(z) = 0 \end{cases} \end{aligned} \quad (11)$$

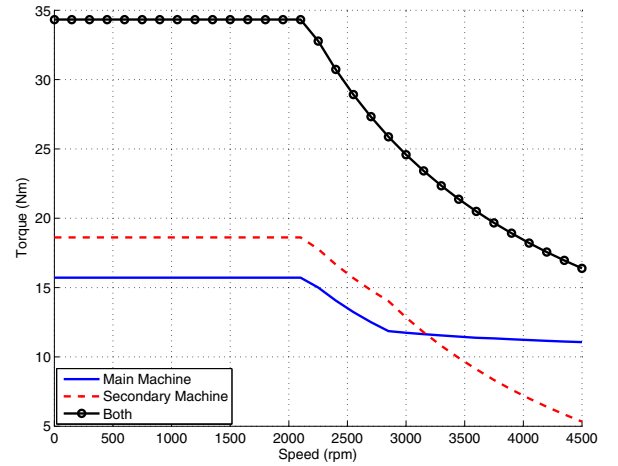
In relation (11), $f_T(z)$ is the constraint relative to the torque, simply obtained by dividing the required constant

electromagnetic power P_{em} by mechanical speed Ω_m :

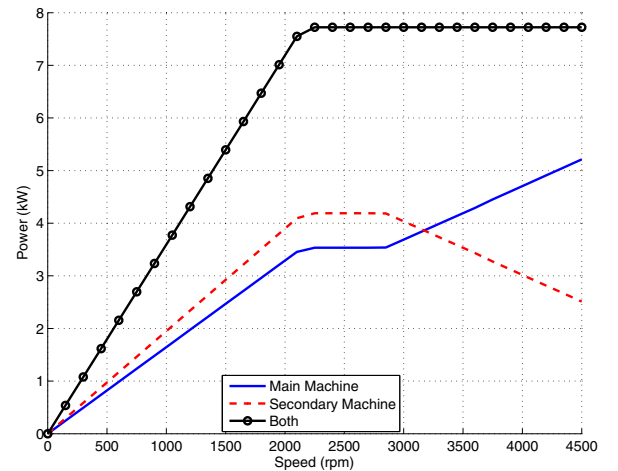
$$f_T(z) = T(z) - \frac{P_{em}}{\Omega_m} \quad (12)$$

The speeds where the CPR can be achieved are deduced from the maximum torque/speed characteristic estimated in the previous subsection (2250rpm - 4500rpm).

Fig.6a shows the obtained torque/speed characteristics: at low speed (below 2250rpm), the reported characteristic is the one according to the MTPA strategy (10) whereas, at high speed, the reported characteristic is the one corresponding to the resolution of the CPR problem (11) introduced in this subsection. Again the torque repartition between the two virtual machines confirms the electronic pole changing effect: at low speed, the SM is mainly used whereas, at high speed, the MM becomes predominant. Fig.6b gives the corresponding power/speed characteristics. As specified, the CPR is actually obtained between 2250rpm and 4500rpm and the electronic pole changing effect already observed when, looking at Fig.6a, is confirmed.



(a) Torque vs speed



(b) Em power vs speed

Fig. 6. Torque and power with CPR-MTPA strategy

B. Constant Power Control with favoring Main Machine

In order to reinforce the pole changing effect at high speed, the constant power control (between 2250rpm and 4500rpm) is calculated so that the Main Machine torque contribution is maximized (always accounting the maximum allowable peak voltage). With this strategy, a limitation of the magnet eddy current losses is expected because the Main Machine owns 0.5 slot per pole and per phase [6]. This strategy is called CPR-h1 and is obtained by solving the following optimization problem:

$$\begin{aligned} z^* &= \operatorname{argmin}(-T_1(z)) \\ \text{with } &\begin{cases} Z_{low} \leq z \leq Z_{up} \\ f_V(z) \leq 0 \\ f_T(z) = 0 \end{cases} \end{aligned} \quad (13)$$

In (13), T_1 denotes the torque produced by the Main Machine defined by (4).

Fig.7a and Fig.7b show respectively the resulting torque/speed and power/speed characteristics when solving optimization problem (13) at high speed (at low speed, below 2250rpm, the MTPA characteristic is given). As aimed for, the torque produced by the Main Machine is maximized in the Constant Power Range. One can observe that, between 3200 and 4200rpm, the Secondary Machine operates in generator mode to facilitate the Main Machine power increase.

C. Losses analysis

Copper, magnet and iron (stator and rotor) losses are now considered with FE software *Ansys Maxwell*. Magnet and iron losses are estimated from the time variation of the flux density. The method to calculate the hysteresis, eddy current and excess losses is close to the one detailed in [16]. For speed belonging to the CPR, the five-phase machine is simulated for the optimized currents corresponding to the CPR-MTPA and CPR-h1 strategies.

Fig.8a and Fig.8b give the copper, magnet and iron losses according to the speed for the CPR-MTPA and the CPR-h1 strategies respectively. With the CPR-MTPA strategy, as aimed for, the copper losses are minimized but, in Fig.8a, it can be observed that copper losses do not represent the major losses. This trend is all the truer as the speed increases. Referring to the CPR-MTPA strategy that allows the lowest copper losses, the CPR-h1 strategy allows to reduce the whole losses up to 3200rpm as shown by Fig.8b. This advantage is based on the significant decrease of the magnet losses. This result complies with the analysis carried out in [8] where it is shown that the asynchronous space harmonics due the third harmonic generate eddy currents in the magnet layer. For SPM machine, magnet losses mitigation is critical because the magnet layer can not be cooled as easily as the stator winding. In steady state, the magnet losses should be carefully controlled to prevent from demagnetization due to overheating.

Fig.9 gives another insight of the possible losses reduction with the CPR-h1 strategy: the efficiency versus speed for the

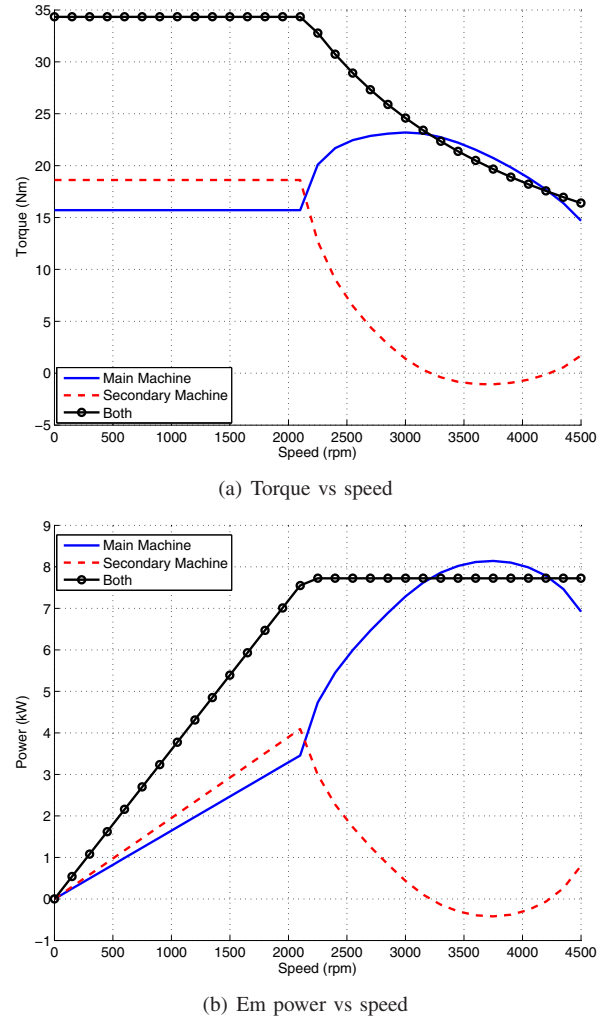
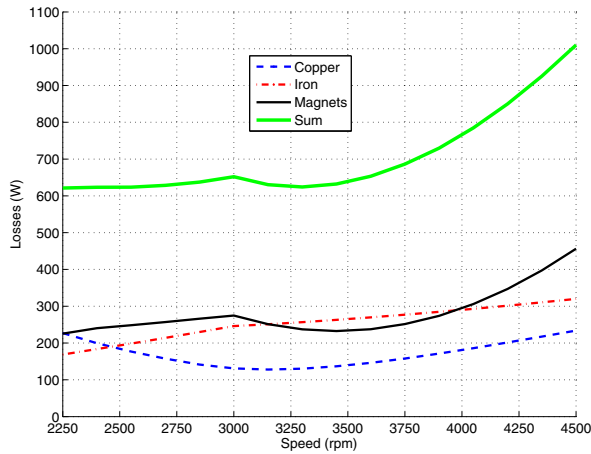


Fig. 7. Torque and power with CPR-h1 strategy

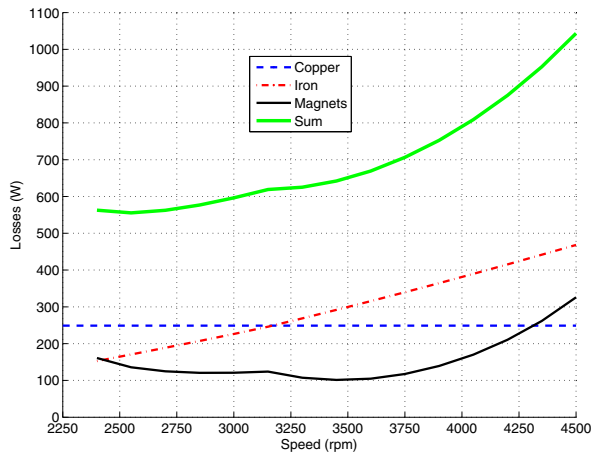
two strategies are represented. Thus the efficiency enhancement up to 3200rpm with the CPR-h1 strategy is illustrated. Finally, for the SPM 20-8-5 machine, the MTPA strategy is not the right solution to maximize the efficiency and to limit the heating of the magnets.

V. CONCLUSION

In this paper, the estimations of the 20-8-5 machine performances are obtained without considering magnetic saturation and demagnetization issue. With a particular but quite simple design of the magnet layer, the 20-8-5 machine inherently owns 3×4 pole pairs and 4 pole pairs. With a single stator and single rotor structure, a magnetic gear behavior is then obtained by controlling two rotating fields. The torque/speed characteristic calculated by considering the current and voltage limitations imposed by the inverter confirms the electronic pole changing effect: at low speed, the SM (3×4 poles) mainly contributes to the torque whereas, at high speed, the MM (4 poles) torque becomes higher. As the propeller is specified to operate in the constant power range



(a) With CPR-MTPA strategy (11)



(b) With CPR-h1 strategy (13)

Fig. 8. Losses according to the speed in the CPR

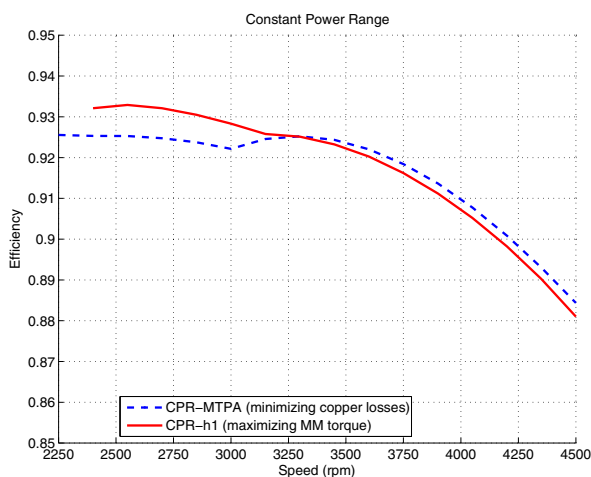


Fig. 9. Efficiency in the CPR for the two strategies

at steady state (between 2250rpm and 4500rpm), the machine losses are numerically estimated for two CPR control strategies: the CPR-MTPA that minimizes the copper losses and the CPR-h1 that favors the MM torque contribution. A better efficiency is obtained with CPR-h1 control up to 3200rpm, with a significant reduction of the magnet losses for the whole speed range. Finally, for the 20-8-5 machine here considered, the existence of an optimal Maximum Torque Per Losses (MTPL) strategy is then demonstrated and have to be explored in further studies.

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